

PROGRAMMABLE TRANSMIT SCSI EQUALIZATION

Field of the Invention

The present invention relates to a method and/or
5 architecture for implementing transceivers generally and, more
particularly, to programmable transmit SCSI equalization.

Background of the Invention

Referring to FIG. 1, a schematic of a conventional
current mode small computer systems interface (SCSI) universal low
voltage differential (ULVD) driver 10 is shown. The driver 10 has
a number of transistors labeled A-D, a driver 12, a current source
14, a current source 16, a positive output pin 18, a negative
output pin 20 and a terminator 22. Input data is presented to the
15 transistors A and C and the transistors B and D in a differential
configuration. Conventional current mode SCSI ULVD drivers do not
control output rise time of output differential waveforms.

It is generally desirable to provide a method and/or
architecture that may overcome SCSI cable induced effects by

01-050
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providing a controlled rise time and synchronized buffers for precompensation.

Summary of the Invention

5 The present invention concerns an apparatus comprising a first plurality of parallel switches and a second plurality of parallel switches. The first plurality of parallel switches may be configured to control a first voltage on a first output pin. The second plurality of parallel switches may be configured to control a second voltage on a second output pin. The first and second pluralities of parallel switches may be configured to provide rise time control of a differential waveform and be driven by a phased data signal.

10 The objects, features and advantages of the present invention include providing a method and/or architecture for a programmable transmit SCSI equalization device that may (i) provide controlled rise time and/or (ii) provide synchronized buffers for precompensation.

Brief Description of the Drawings

These and other objects, features and advantages of the present invention will be apparent from the following detailed description and the appended claims and drawings in which:

5 FIG. 1 is a block diagram of a conventional SCSI ULVD driver;

FIG. 2 is a block diagram of a preferred embodiment of the present invention;

FIG. 3 is a block diagram of an alternate embodiment of the present invention;

FIG. 4 is a block diagram of an exemplary implementation of the present invention;

FIG. 5 is a block diagram of a clock generation circuit in conjunction with the present invention;

15 FIG. 6 is a timing diagram of the circuit of FIG. 5;

FIG. 7 is a timing diagram of an operation of typical bandwidth effects over a transfer medium without pre-emphasis;

FIG. 8 is a timing diagram of an operation of the present invention;

20 FIG. 9 is a block diagram of an alternate embodiment of the present invention; and

01-050
1496.00128

FIG. 10 is a block diagram of a timing circuit of the circuit of FIG. 9.

Detailed Description of the Preferred Embodiments

5 Referring to FIG. 2, a block diagram of circuit (or device) 100 is shown in accordance with a preferred embodiment of the present invention. The circuit 100 may be implemented as a small computer systems interface (SCSI) universal low voltage differential (ULVD) transceiver. The circuit 100 may provide a SCSI ULVD driver with precompensation and rise time control. The circuit 100 may be implemented to control rise and fall times with phased data. For example, the circuit 100 may provide controlled rise time of low voltage differential signals in a SCSI ULVD buffer. The circuit 100 may be configured to provide minimized rise time variation of differential drivers over process, voltage, and temperature corners. Additionally, the present invention may provide synchronization of multiple differential drivers (to be described in connection with FIGS. 3 and 4).

The circuit 100 generally comprises a circuit (or device) 102, a circuit (or device) 104, a current source 106, a current source 108, a terminator 110, and an inverter 112. The circuit 100

01-050
1496.00128

may also have an output pin (e.g., V+) and an output pin (e.g., V-). The circuit 102 generally comprises a number of parallel switches (e.g., A) and a number of parallel switches (e.g., C). The parallel switches A<1:N> and the parallel switches C<1:N> may
5 be driven by a data signal (e.g., DATA). The data signal DATA may be a phased data signal with N phases, where N is a positive integer. The circuit 104 generally comprises a number of parallel switches (e.g., B) and a number of parallel switches (e.g., D). The parallel switches B<1:N> and the parallel switches D<1:N> may
10 be driven by a complement of the phased data signal DATA. A number of each of the parallel switches A, B, C and D may be varied in order to meet the criteria of a particular implementation.

The switches A, B, C and D may be implemented as ULVD rise time control switches. The circuit 100 may implement rise
15 time control by implementing N parallel switches (e.g., the switches A<1:N>, B<1:N>, C<1:N> and D<1:N>) driven by a phased data signal (e.g., the signal DATAN). The circuit 100 may break the output switches A, B, C and D in to multiple segments and drive them with the multiphase data signal DATAN. The timing between a
20 first and a last data phase (e.g., DATA1 and DATAN) of the signal DATA may determine rise and fall times of an output differential

01-050
1496.00128

waveform on the pins V+ and V-. The switches A, B, C and D may also be weighted to influence a pulse shape of the differential waveform.

Referring to FIG. 3, a block diagram of a circuit 180 illustrating an exemplary embodiment of the circuit 100 is shown. The circuit 180 may be similar to the circuit 100. The circuit 180 may be configured to synchronize multiple buffers. The circuit 180 may allow phased data to be created from a centrally generated phased clock. The circuit 180 may also allow two differential devices to become synchronized by a common phased clock (to be discussed further in connection with FIG. 4). The circuit 180 may additionally comprise a flip-flop 150 and a flip-flop 152. The flip-flops 150 and 152 may be implemented as output driver switches. The FF 150 may receive a signal (e.g., I1). The FF 152 may receive a signal (e.g., I1b). The FFs 150 and 152 may also receive a clock signal (e.g., CLOCK). The clock signal CLOCK may be implemented as a multiphase clock signal.

Referring to FIG. 4, a block diagram of a circuit (or device) 190 illustrating an exemplary implementation of the present invention is shown. The circuit 190 generally comprises a driver 180a and a driver 180b. The circuit 190 may illustrate a

01-050
1496.00128

precompensation implementation of the present invention. The drivers 180a and 180b may be similar to the driver 100 (or 180). The drivers 180a and 180b may be configured to line up timing between the output pins V+ and V-. The driver 180a may be implemented as a main driver and the driver 180b may be implemented as a secondary driver. For example, SCSI Ultra4 I/O may require two parallel drivers (e.g., the driver 180a and 180b) in order to perform pre-emphasis on transmitted data. The drivers 180a and 180n may provide pre-emphasis that may mitigate the effects of intersymbol interference (ISI). The signal I1 may be implemented as data signal. The signal I2 may be implemented as a precompensation signal of the signal I1.

In order to synchronize the timing, on the drivers 180a and 180b, the circuit 190 may implement the flip-flops 150 and 152. The multiphase clock CLOCK<1:N> may drive both the main driver 180a and the secondary driver 180b. However, the clock CLOCK<1:N> may be implemented to drive any number of buffers. The multiphase clock CLOCK<1:N> may be implemented to create a multiphase data pattern to the output driver switches.

The circuit 190 is shown comprising two drivers (e.g., the drivers 180a and 180b). However, another appropriate number of

01-050
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drivers may be implemented to meet the criteria of a particular implementation. Additionally, for a higher number of drivers 180a-180n implemented in the circuit 190, higher orders of precompensation may be achieved.

5 Referring to FIG. 5, a block diagram of a timing device (or circuit) 200 is shown. The timing circuit 200 may be used in conjunction with the present invention to generate the multiphase clock signal CLOCK<1:N>. The timing circuit 200 may also be configured to control rise time variation. The circuit 200 may generate clock phases from an edge transition on either the data signal I1 or the precompensation signal I2.

10 The timing circuit 200 generally comprises a delay device 202, a gate 204, a delay device 206, a gate 208, a gate 210, a latch 212, an inverter 213, a number of clock phase generation circuits 214a-214n, an inverter 216 and a bias circuit 218. A
15 number of clock phase generation circuits 214a-214n may be varied in order to meet the criteria of a particular implementation. The gates 204 and 208 may be implemented as XNOR gates and the gate 210 may be implemented as an AND gate. However, other types of gates
20 may be implemented in order to meet the design criteria of a particular implementation.

01-050
1496.00128

The data signal I1 may be presented to the delay circuit 202 and the gate 204. The gate 204 may also receive an output of the delay circuit 202. The precompensation signal I2 may be presented to the delay circuit 206 and the gate 208. The gate 208 may also receive an output of the delay 206. The gate 204 and the gate 208 may present a signal to the gate 210. The gate 210 may present a signal to a set input of the latch 212. The latch 212 may present an output signal to the inverter 213 and the clock phase generation circuit 214a. The inverter 213 may generate the clock signal CLOCK<1>.

The clock phase generation circuits 214a-214n may be coupled in a series configuration. The clock phase generation circuits 214a-214n may be configured to generate the signals CLOCK<2:N>. The clock signal CLOCK<N> may be presented to the inverter 216. The inverter 216 may then present a signal to a reset input of the latch 212. The latch 212 may be configured to control the phases of the clock CLOCK<1:N> via the phase clock generation circuits 214a-214n. Additionally, the bias circuit 218 may be configured to control the circuit 214a-214n. The bias circuit 218 may be controlled by a signal (e.g., IBIAS).

01-050
1496.00128

Each of the clock phase generation circuits 214a-214n generally comprises a transistor 220, a transistor 222, a transistor 224, an inverter 226 and an inverter 228. A source of the transistor 220 may be coupled to a power supply, a gate of the transistor 220 may be coupled to a proceeding output, and a drain of the transistor 220 may be coupled to a source of the transistor 222. A gate of the transistor 222 may be coupled to the proceeding output and a drain of the transistor 222 may be coupled to a source of the transistor 224. A gate of the transistor 224 may receive a bias output of the bias circuit 218 and a drain of the transistor 224 may be coupled to ground.

The inverter 226 may receive the drain of the transistor 220/the source of the transistor 222. The inverter 226 may present a signal to a next clock phase generation circuit. The inverter 228 may receive the output of the inverter 226 and present a phase of the signal CLOCK.

The timing circuit 200 may synchronize multiple differential drivers with a centralized delay line to generate the multiphase clock CLOCK<1:N> from data edge transitions. The multiphase clock CLOCK<1:N> may then drive an array of flip-flops (e.g., the flip-flops 150 and 152) to generate the differential

01-050
1496.00128

waveform output on the pins V+ and V-. Additionally, the timing circuit 200 may implement a PLL (or DLL) to create the multiphase clock delay line bias current IBIAS. However, other appropriate clock generation techniques may be implemented.

5 The timing circuit 200 may be configured to provide edge rate control. The circuit 100 may also allow the timing circuit 200 to be implemented for multiple transmitters. The timing circuit 200 may also allow for the precise synchronization of several outputs and several parallel transmitters to be precisely
10 synchronized for multi-level transmit.

Referring to FIG. 6, a timing diagram 300 illustrating an operation of the timing circuit 200 is shown. A time from a transition of the signal CLOCK<1> to a transition of the signal CLOCK<N> may set the rise and fall times for each differential
15 output stage 214a-214n and may be controlled by the current source IBIAS. For example, in SCSI Ultra4, the control signal IBIAS may be a process, voltage, and temperature (PVT), compensated source providing 1.5:1 delay variation. The PVT compensation may be adjusted with control bits from about 40 μ A to 80 μ A. Additionally,
20 the signal IBIAS may be designed to further track PVT variation by using a PLL (or DLL) with a delay in the control loop being

01-050
1496.00128

composed of the delay circuits 202 and 206. The signal CLOCK<1> be delayed from the signals I1 and I2 to provide sufficient set-up time on the flip-flops 150 and 152. However, the signal CLOCK<N> may not be delayed beyond a hold-time of the flip-flops 150 and
5 152.

Referring to FIG. 7, a timing diagram 500 of a typical transmission operation without pre-emphasis is shown. The timing diagram 500 may illustrate the eye of data transmitted over 25 meters of cable. The timing diagram 500 may illustrate the bandwidth-limiting effects (ISI) of the cable on data transmitted without pre-emphasis.
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Referring to FIG. 8, a timing diagram 600 illustrating an operation of the present invention is shown. The timing diagram 600 may illustrate the eye of data transmitted over 25 meters of cable with pre-emphasis. The timing diagram 600 may have a significant improvement in ISI distortion with respect to the timing diagram 500.
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Referring to FIG. 9, a block diagram of a circuit 100' is shown illustrating a five phase SCSI driver. The circuit 100' may be similar to the circuit 100. The circuit 100' may comprise a number of current sources 106a-106n and 108a-108n and a number of
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01-050
1496.00128

flip-flops 150a-150n and 152a-152n. A number of current sources 106a-106n, current sources 108a-108n, flip-flops 150a-150n and flip-flops 152a-152n may be varied in order to meet the criteria of a particular implementation. The current sources 106a-106n and 108a-108n may be weighted to influence pulse shapes of the differential waveform. The switches A, B, C and D may also be weighted. In one example, the circuit 100 may implement the individual current sources 106a-106n and 108a-108n and the equally weighted switches A, B, C, and D to control current switching. The circuit 100' may also implement a number of clock phases (e.g., CL1, CL2, CL3, CL4 and CL5).

The current sources 106a-106n may be implemented as P-channel current sources. The switches A and B may be implemented as P-channel switches. The current sources 108a-108n may be implemented as N-channel current sources. The switches C and D may be implemented as N-channel switches. In one example, each of the current sources 106a-106n and 108a-108n may be implemented as a 2mA current source. However, the particular size of the current sources 106a-106n and 108a-108n may be varied accordingly to meet the design criteria of a particular implementation. Additionally,

01-050
1496.00128

the current source 106a and the current source 108a may act as offset cancellation current sources.

In one example, five switches with equal weighting and combined current sources are typically implemented for SCSI Ultra3. SCSI Ultra3 I/O devices may control rise time with a 3:1 variation across PVT. In another example, five switches with binary (e.g., 1,2,4,2,1) weighting may be implemented for SCSI Ultra4. SCSI Ultra4 may implement binary switch weighting to open the eye (to be discussed in connection with FIGS. 7 and 8). SCSI Ultra4 may also use a current controlled delay line for generation of multiphase data. The current controlled delay line may provide 1.5:1 variation across PVT. Such an implementation may improve operation of conventional SCSI Ultra4 devices.

Referring to FIG. 10, a circuit 200' is shown. The circuit 200' may be similar to the circuit 200. The circuit 200' may be configured to generate the clock phases CL1-CL5. The circuit 200' may generate the clock phases CL1-CL5 in response to the signal DATA. The clock generation circuit 200' may trigger on data transitions of the signal DATA.

Conventional LVD transmitters in multi-drop cable environments require edge-rate control to avoid generation of

01-050
1496.00128

crosstalk and reflection noise. However, such conventional solutions are configured to slow down the output data at the output (or last) stage for a timed transition at the output. The circuit 100 may be configured to separate the timing for LVD edge-rate control out of the critical data path. Specifically, the timing circuit 200 may not be implemented in the critical data path. Therefore, the timing circuit 200 may not delay the output differential waveform of the circuit 100. The circuit 100 may detect when the output on the pins V+ and V- is about to change state and trigger the timing circuit 200 to control the transmitted edge rate.

The circuit 100 may implement the parallel drivers 180a and 180b to improve transmitter ISI precompensation. The circuit 100 may also implement the parallel weighted current sources 106a-106n and 108a-108n to improve ISI precompensation. The circuit 100 may implement weighted switching to improve the transition levels in the current-mode driver 100 (or 190). The overall impedance of the switches A, B, C and D may be set by a predetermined common-mode range requirement. The individual impedance of each switch A, B, C, and D may be optimized, such that when turning on the total resistance of all switches N, at a particular point

01-050
1496.00128

changes by $1/N$. The circuit 100 may therefore avoid a case when first and last switch are small compared to the termination resistance.

5 While the invention has been particularly shown and described with reference to the preferred embodiments thereof, it will be understood by those skilled in the art that various changes in form and details may be made without departing from the spirit and scope of the invention.